

MIDDLE EAST TECHNICAL UNIVERSITY

Electrical & Electronics Engineering

Hardware Project

EE 464 – Static Power Conversion - II

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Table of Contents

[Introduction 1](#_Toc10469609)

# Introduction

In our hardware project of the EE464 course, we are asked to design an Isolated Power Supply. In this project, the design, simulations and hardware implementations are to be performed for hardware project. As Anka Inc. group, we have chosen the project designing an Isolated Flyback Converter. The specifications are as follows;

|  |  |
| --- | --- |
| Minimum Input Voltage (V) | 210 Vac |
| Maximum Input Voltage (V) | 230 Vac |
| Output Voltage (V) | 15 |
| Output Power (W) | 15 |
| Output Volt. Peak-to-Peak Ripple (%) | 5 |
| Line Regulation (%) | 3 |
| Load Regulation (%) | 3 |

Table 1: Flyback Converter Specifications

The main motivation selecting this topology is to overcome efficiency problems as our output current value is smaller, which results in less power loss in overall system. Also, there is no 3rd winding in transformer designed for Flyback Converter as well as output inductance for filtering purposes as in Forward Converter topology.

# 1. Flyback Converter Design

Our input voltage is AC voltage with 210 Vrms. Firstly, we establish the single phase full bridge rectifier to convert AC to DC and the DC voltage is filtered by DC-Link Capacitor. Then, a Flyback Converter is established by PI controller. PI controller is required to adjust the output power 15 V for not considering input voltages change.

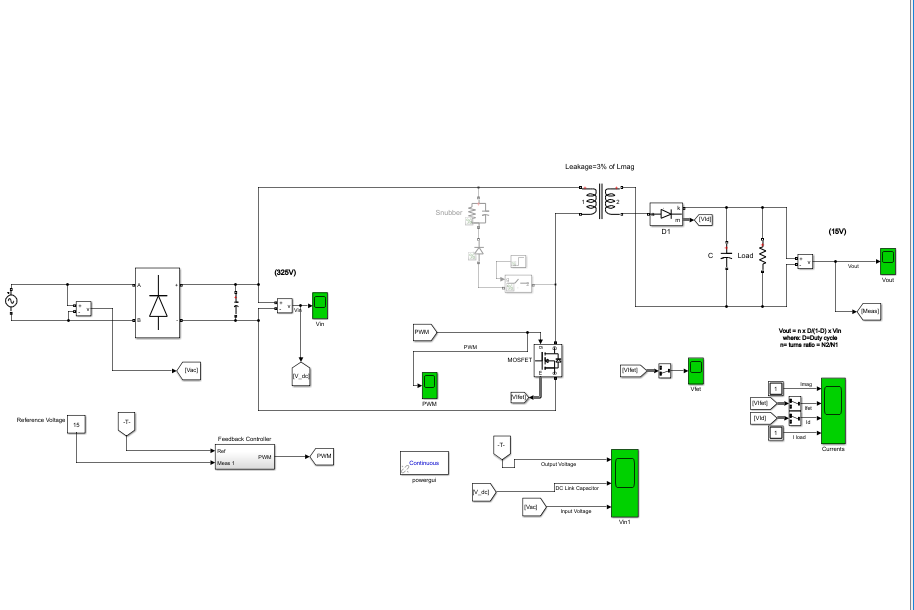


Figure 1: Simulink Setup of Flyback Converter

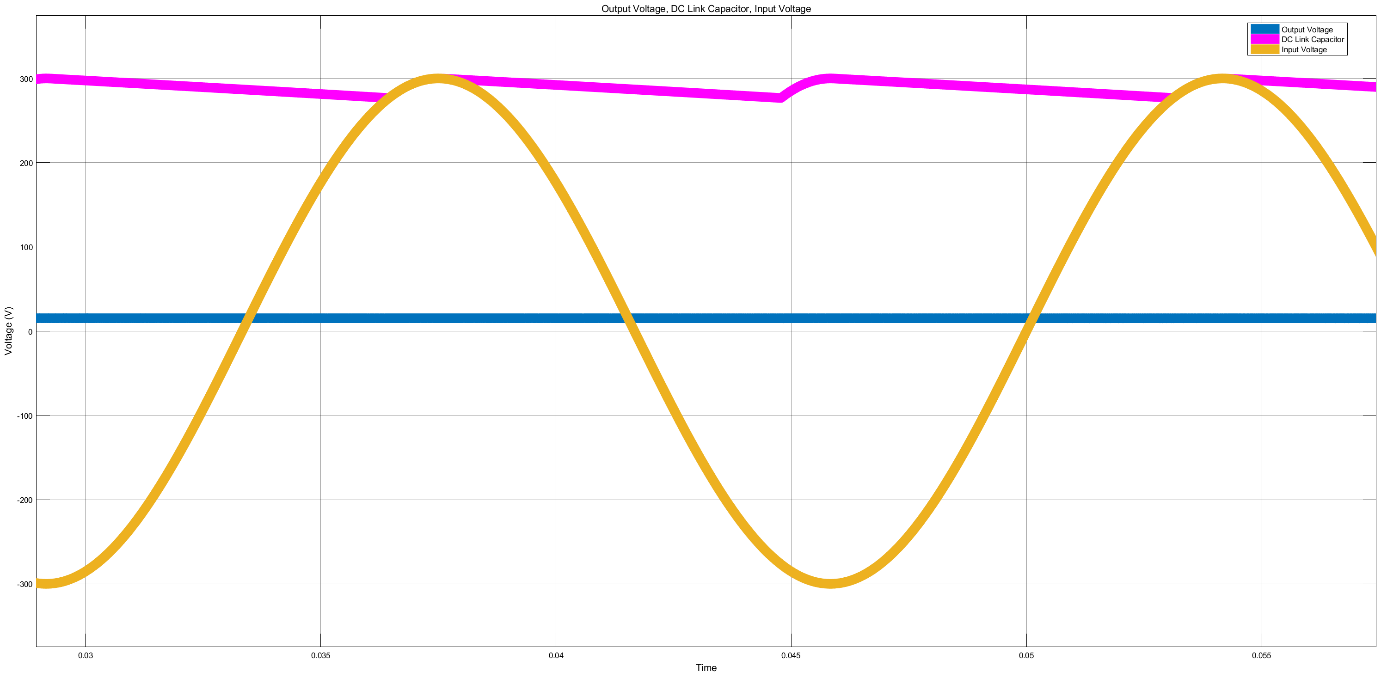


Figure 2: Inputs and Output Voltages of the Flyback Converter

## 1.1. Steady State Operation and Calculations

There are 5 steps to calculate the parameters to provide specification:

1. DC link capacitor determination for Single Phase Rectifier:

DC link capacitor is determined by AC voltage and frequency with desired ripple at output of the single phase rectifier.

The DC link capacitor is calculated easily as 33uF, 400 V.

1. Magnetizing Inductance is calculated by formula:

Maximum duty can be selected for mode of converter. We want our converter to operates at discontinuous conduction mode. Thus, standard duty ratio is near the 0.3. Maximum duty is 0.45. Ripple factor (Krf) is 1 at DCM and it is between 0.2 and 0.5 at CCM. Switching frequency was determined as 40 kHz.

1. Calculation of Peak Current of Switch

The calculation is important to determine the CCM and DCM mode. Change in switch current is equal to half of peak current or equals to I\_eds.

1. Determination of primary side Turn number

Minimum turn number depends on core. The core area and saturation flux density.

They are found at our core datasheet.

1. Determination of primary side Turn number

Secondary side turn ratio depends on primary side voltage and secondary side voltage. Secondary side voltage includes output voltage and opening voltage of diodes.

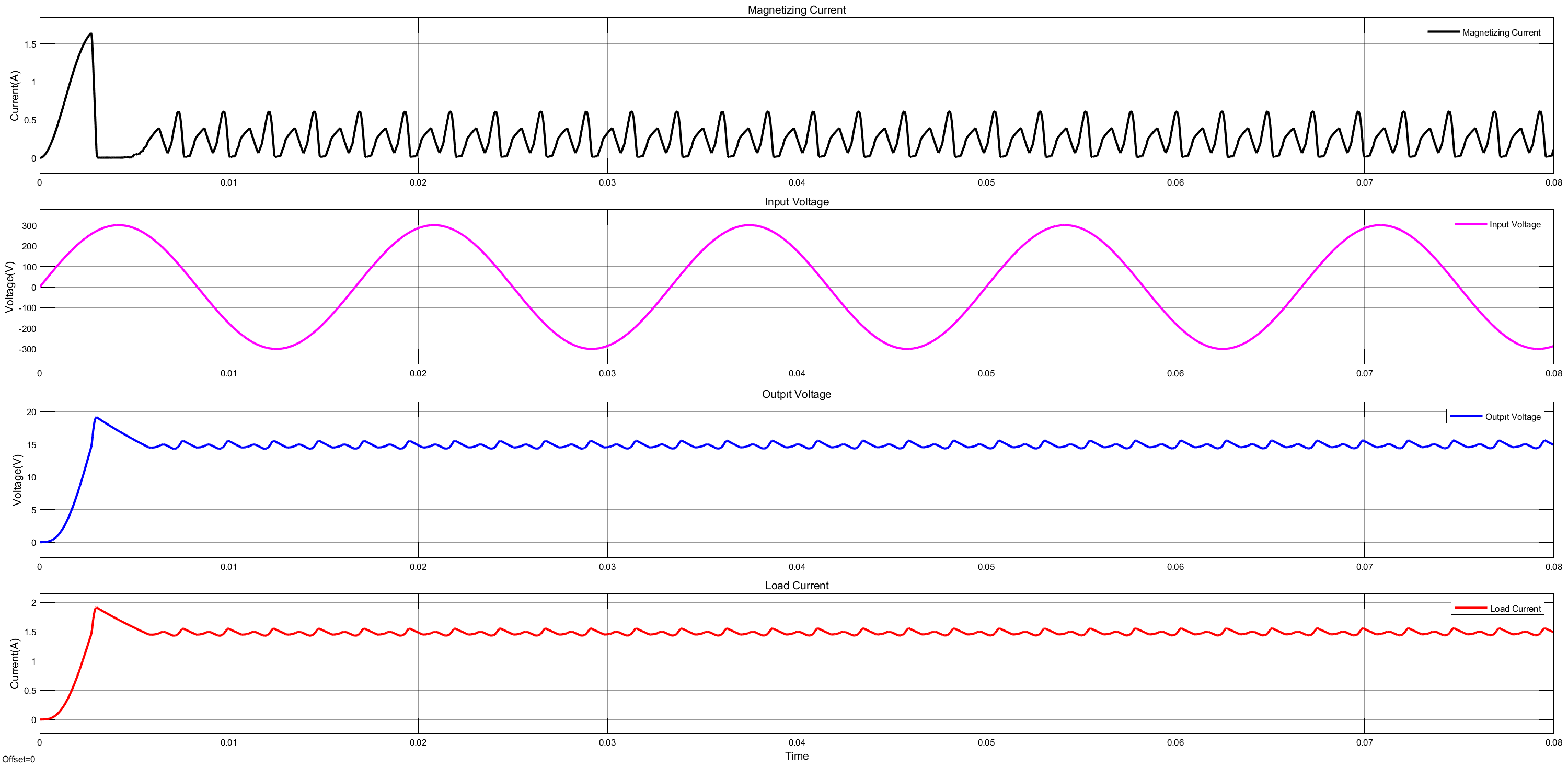


Figure 3: Corresponding waveforms with ideal switches and elements

## 

Leakage inductance is taken as 3 percentage of magnetizing inductance. The MOSFET conduction resistance is 10 ohms, and diode conduction resistance is 5 ohms. Switch Voltage and Switch current are taken at only conduction time.

Without Snubber Circuit:

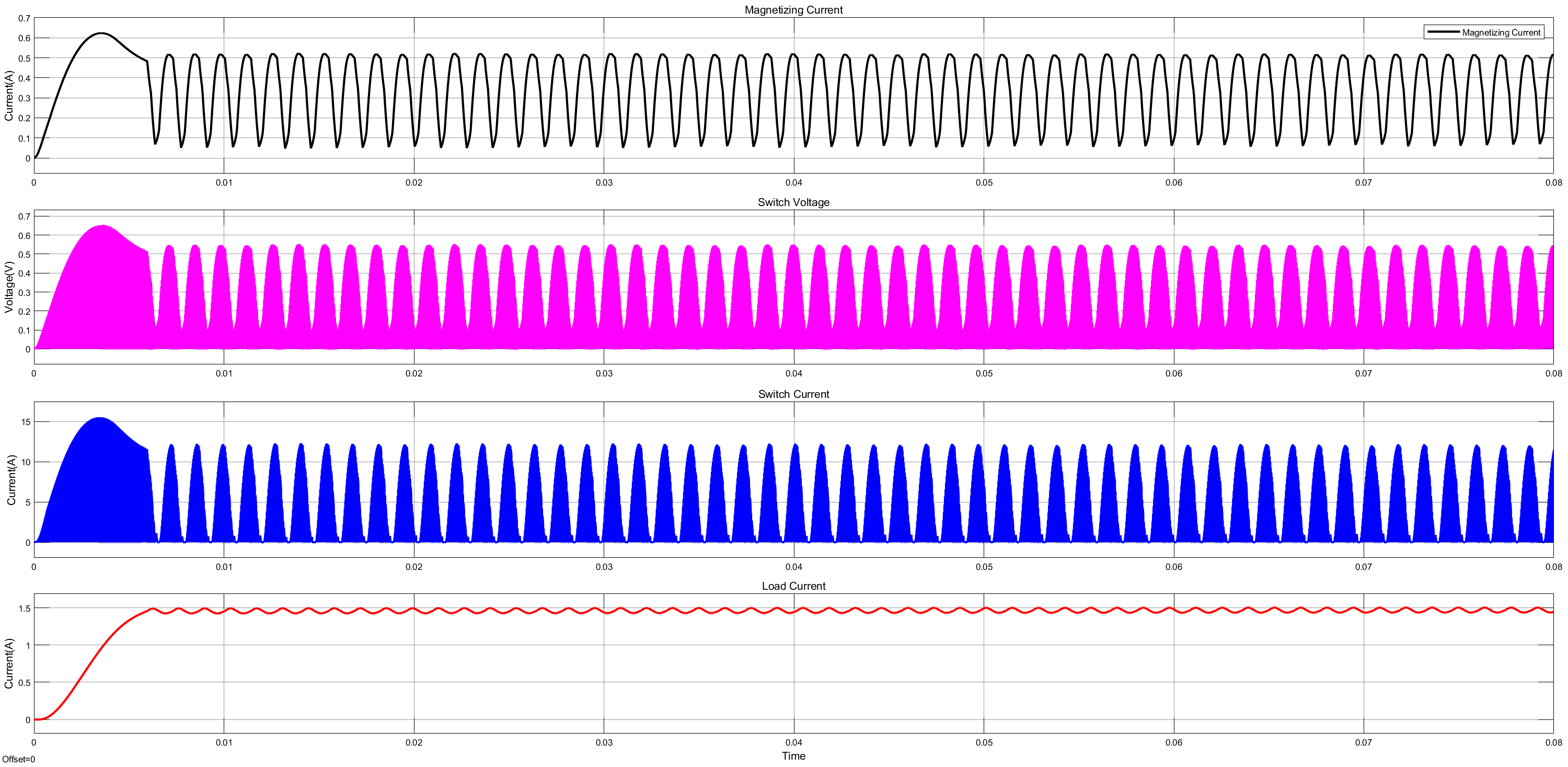


Figure 4: Corresponding waveforms without snubber circuit

With Snubber Circuit:

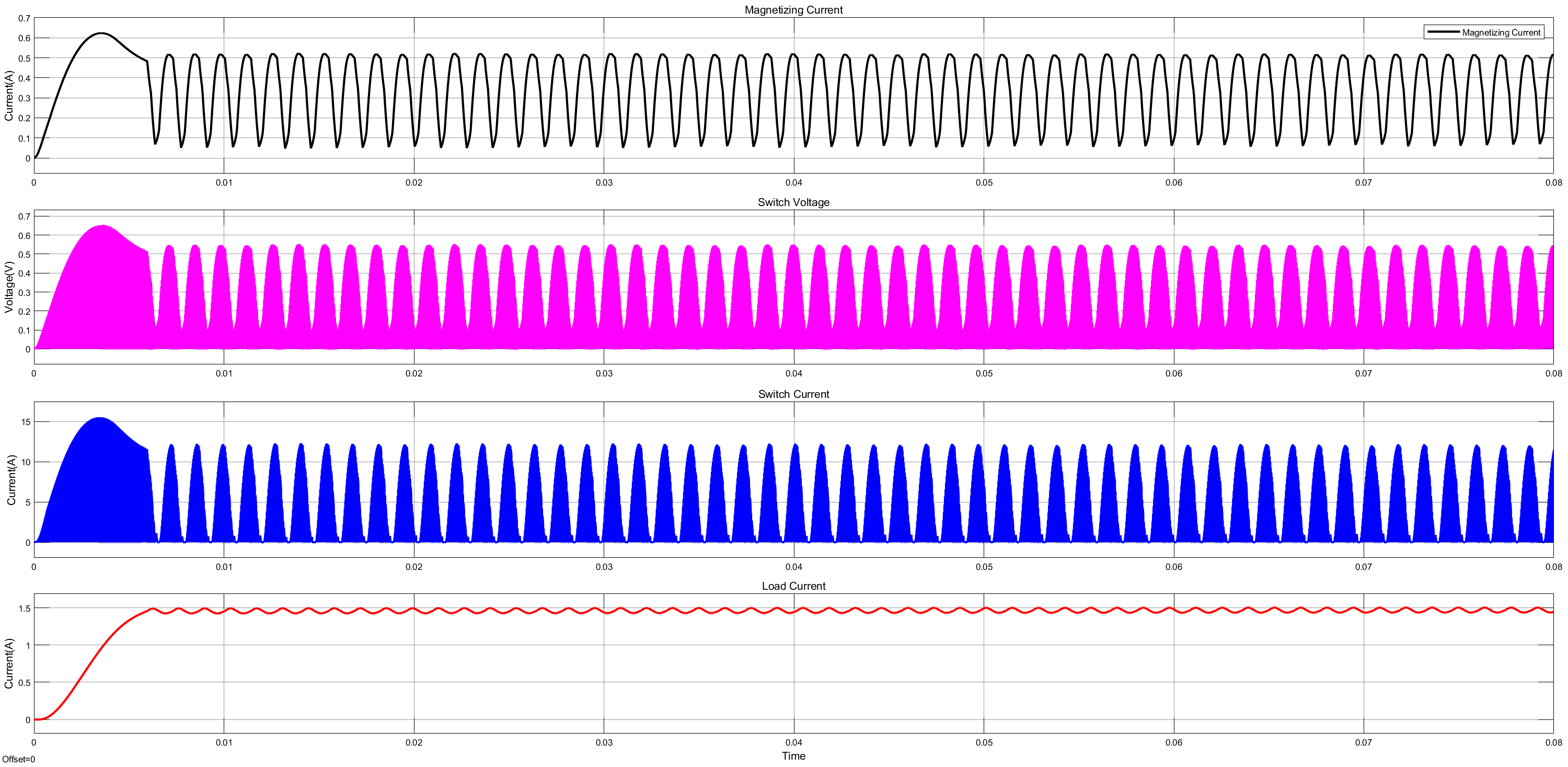


Figure 5: Corresponding waveforms with snubber circuit

Without snubber circuit, the energy storage is not transferred to load. Load current decreases and output voltage is not provided successfully.

RCD snubber circuit is established. The value of components is found considering switching frequency and time constant RC of the snubber circuit.

R=40k ohm

C= 100 pF

## 1.2. Transformer Design

At this part, we are supposed to design a transformer for our Flyback Converter. There are some properties that are important for designing such as permeability, saturation flux and core loss. Geometry and core type of the transformers determines the properties.

Transformer geometry toroid changes with respect to applications and some geometries are E-core I-core and Toroid core. E- cores are easier to wind and mount by using transformer core former. We chose the core geometry as E-core for that reason. Saturation flux depends on current ratings. Our current rating is small, 1A and we can choose saturation flux density as small. Also, permeability affects the magnetizing inductance which is very important to Flyback design because transformer is used for energy storage elements in Flyback. In addition to this, core loss is very important to determine switching frequency because of the efficiency consideration.

We, as Anka Inc. Team, made a Matlab Script to determine the design parameters with respect to our requirements. The script is given as APPENDIX.

By using this script, we found that:

Requirement Magnetizing Inductance: 10.58mH

Np/Ns= 15 (maximum duty is determined as 0.45) and minimum Np=45 turns

## 1.3. Simulation Results

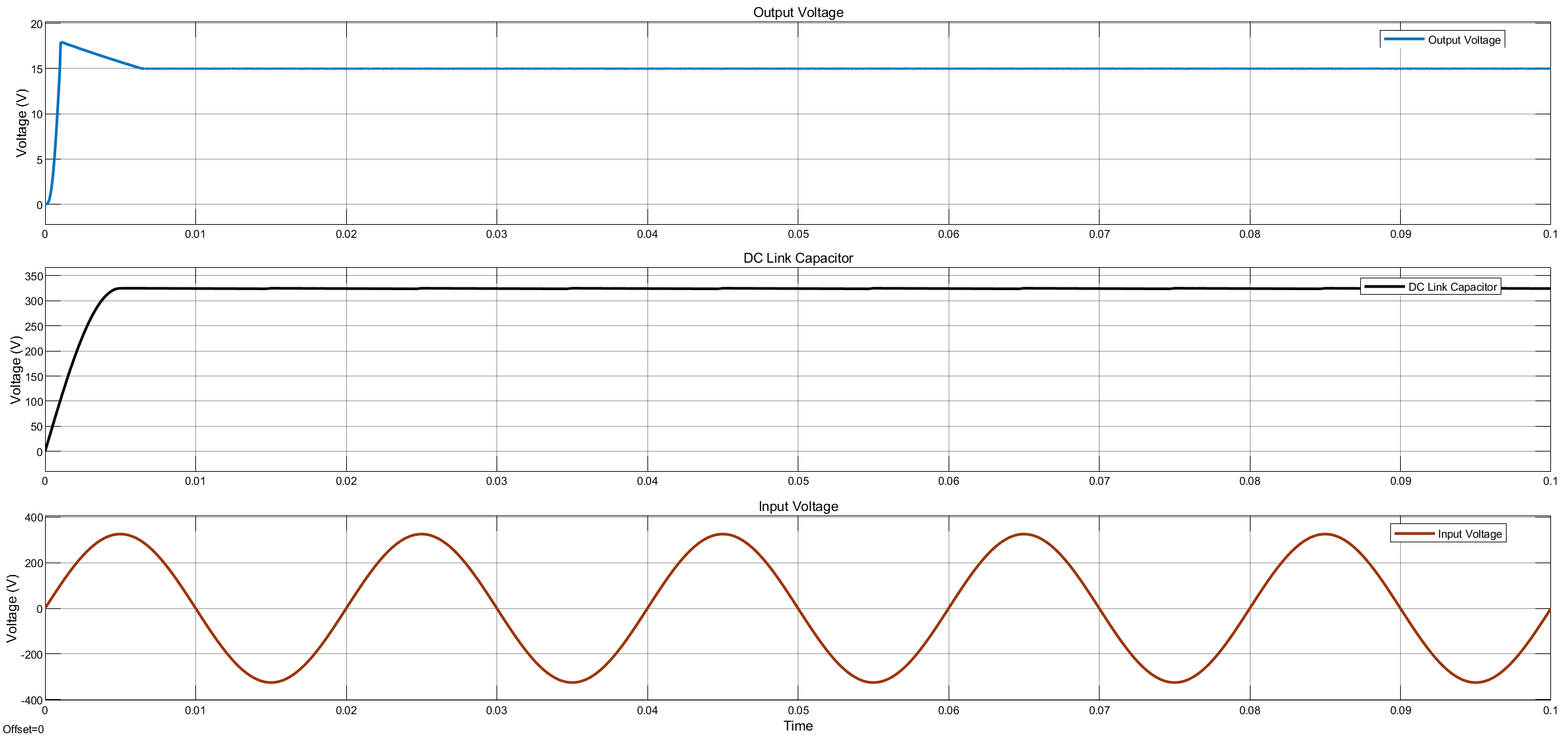


Figure 6: Output, DC Link Capacitor and Input voltage waveforms

With the calculated values and parameters, voltage values are matched with simulation as shown in Figure 6.

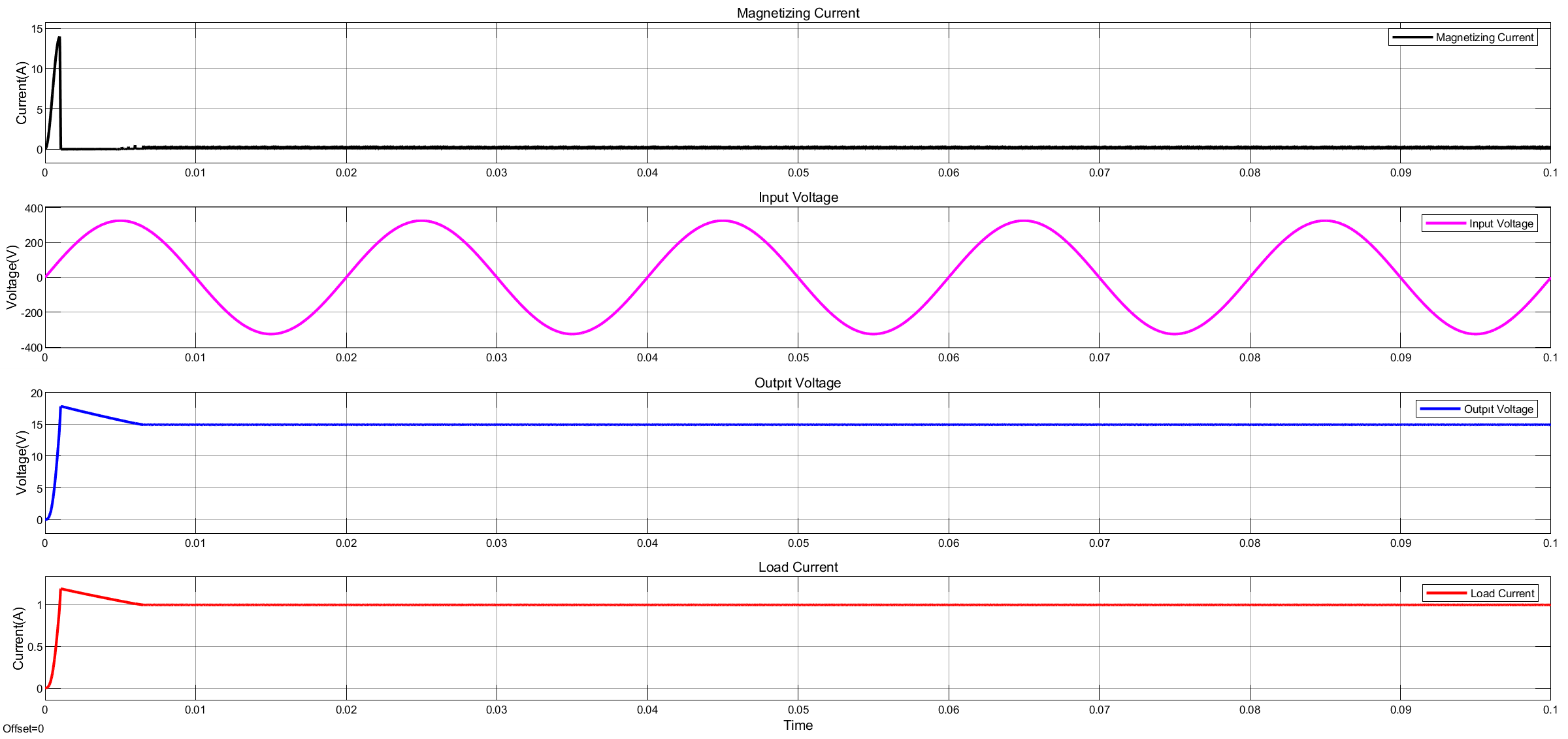


Figure 7: Magnetizing and Output Current waveforms as well as Input and Output Voltages

As shown in Figure 7, the desired voltage and current values are reached. In initial time period, there seems a peaky increase in magnetizing current but it is directly eliminated. Hence, proper operation is proved by simulation results.

|  |  |  |  |
| --- | --- | --- | --- |
|  | Input Power (W) | Output Power (W) | Efficiency (%) |
| %100 | 21.12 | 14.98 | 71 |
| %75 | 17.6 | 11.24 | 63 |
| %50 | 12.1 | 7.48 | 60 |
| %25 | 8.3 | 3.74 | 45 |

Table 2: Efficiency calculation with different load characteristics

As the load is decreased, the efficiency is decreased as shown in Table 2. The reason for that is the losses in transformer stays constant although the changes in output and input powers. Transformer losses have bigger portion in the loss calculations in that case. Therefore, efficiency is decreased with decreasing load. Also, the controller and converters are designed considering %100 load. Therefore, the efficiency is expected to be lower than designed circuit with different load characteristics.

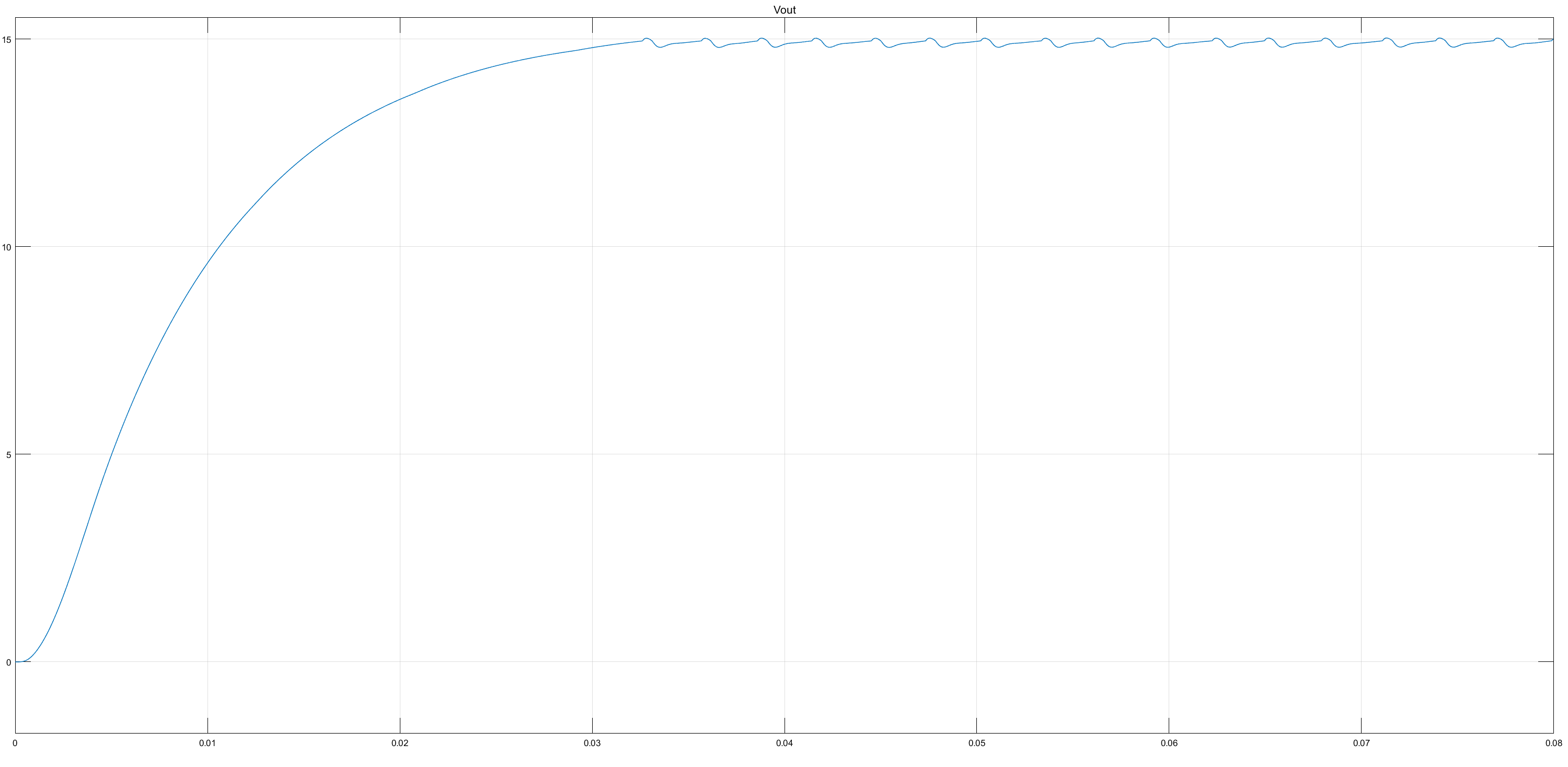


Figure 8: Output waveform with input voltage 210 Vac

%1.3 ripple at 210 Vac is observed in the output voltage waveform which is a reasonable value with desired ripple value less than 5%.

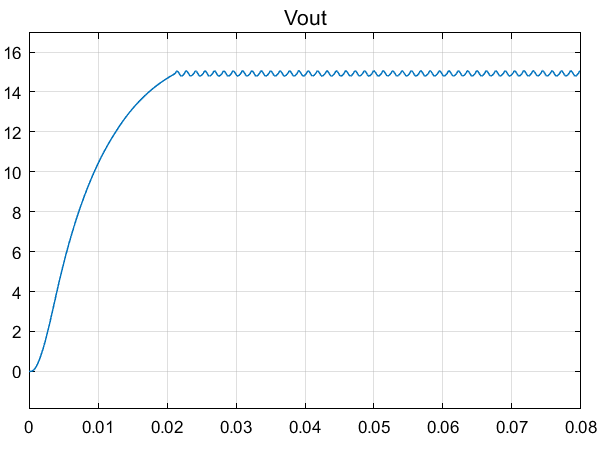


Figure 9: Output waveform with input voltage 230 Vac

%1.6 ripple at 230 Vac is observed in the output voltage waveform which is a reasonable value with desired ripple value less than 5%. Figures 8 and 9 show that the output ripple condition is satisfied with the designed converter design.

## 1.4. Component Selection

### 1.4.1. Transformer

At first we have chosen a core with a bigger transformer area. However, using AWG22 cables, we can reduce the size of transformer which is good for design and implementation. Thus, the final core is chosen as ‘0P43517EC’. It has Kool Mu core and the area of core is 233mm^2. The properties meet our specifications and requirements.

### 1.4.2. Capacitor

### 1.4.3. Diode

### 1.4.4. MOSFET

### 1.4.5. Rectifier Bridge

# 2. Test Results

## 2.1. Overall Design

## 2.2. Transformer Results

## 2.3. RLC Measurement

## 2.4. Output Voltage and Current

## 2.5. Input Voltage

## 2.6. Switching Performance

## 2.7. Efficiency

# Conclusion

# Appendix

%%

clear all;

clc;

%% Flyback Parameters

V\_line\_minimum= 210; % V rms

V\_line\_max=230 ; % Vrms

V\_dc\_min= 280; % 5 percentage ripple

V\_dc\_max=sqrt(2)\*V\_line\_max;

Output\_power= 15; % Watt

Efficiency= 0.8 ; % between 0-1

Input\_power= Output\_power/Efficiency;

%% DC Link Capacitor Calculation

D\_ch=0.2; % for capacitor charging duty

F\_line= 50; % Line frequency

C\_DC = (Input\_power\*(1-D\_ch))/ ...

(F\_line\*((2\*V\_line\_minimum^2)-V\_dc\_min^2));

fprintf(' %f microFarad \n',C\_DC\*1e6);

%% Determination of Maximum Duty Cycle

D\_max= 0.45 ; % for CCM mode, it is bigger than 0.5

V\_Ro= (D\_max/(1-D\_max))\*V\_dc\_min;

V\_ds= V\_dc\_max+V\_Ro;

%% Lm Determination

f\_s= 40000; % Switching Frequecny Hertz

K\_f= 1; % for ccm 0.25-0.50

L\_m= (( V\_dc\_min\*D\_max)^2)/(2\*Input\_power\*f\_s\*K\_f)...

\*1e3; % mili Henry

fprintf('% f mH \n', L\_m);

L\_m=L\_m\*1e-3;

%% Calculation of peak current of FSP( mosfet, IGBT)

I\_edc= Input\_power/(V\_dc\_min\*D\_max); % average ...

... switching amplifier

Delta\_Ids= (V\_dc\_min\*D\_max)/(L\_m\*f\_s);

Ids\_Peak=I\_edc+(Delta\_Ids/2);

Ids\_rms=sqrt((3\*I\_edc^2) + ((Delta\_Ids/2)^2\*D\_max/2));

fprintf('%f %f \n',Ids\_Peak,Ids\_rms);

%% Primary Side Turns Determination

Ae=233\*1e-6; % m^2

B\_sat=0.3 ; %Tesla

N\_p= ((L\_m\*Ids\_Peak)/(B\_sat\*Ae));

fprintf('%f \n', N\_p);

%% Secondary Side Turn Ratio

N\_s= N\_p/((V\_Ro)/(15+0.7));

fprintf('%f \n', N\_s);